TECHNICAL RESEARCH REPORT

Two-Dimensional Spatial Smoothing for Multipath Coherent Signal Identification and Separation

by H. Wang and K.J.R. Liu

T.R. 95-100

Sponsored by the National Science Foundation Engineering Research Center Program, the University of Maryland, Harvard University, and Industry
TWO-DIMENSIONAL SPATIAL SMOOTHING FOR MULTIPATH
COHERENT SIGNAL IDENTIFICATION AND SEPARATION

Hongyi Wang and K. J. Ray Liu

Electrical Engineering Department
Institute for Systems Research
University of Maryland
College Park, MD 20742
Phone: (301) 405-6619

ABSTRACT

The existing spatial smoothing (SS) technique, although it is effective in decorrelating coherent
signals, is considered applicable only to uniformly spaced linear arrays which are very sensitive to
the directions-of-arrival (DOA's) and can be used to estimate azimuth angles only. To significantly
improve the robustness of DOA estimation and of beamforming and to estimate both azimuth and
elevation angles in a 3D multipath mobile radio environment, we developed techniques for applying
SS to arrays of nonlinear geometry. We found and proved the necessary and sufficient conditions on
an array configuration for applying SS. This array must have an orientational invariance structure
with an ambiguity free center array, and the number of subarrays must be larger than or equal
to the size of the largest group of coherent signals. We also studied the cause of ambiguities in a
multipath environment. We found the necessary and sufficient conditions for a three-sensor array
manifold to be ambiguity free and identified several higher order ambiguity situations. If an array
is also central symmetric, the forward/backward spatial smoothing can be used to improve the
resolution. Finally, we expanded the application of our technique not only to MUSIC and adaptive
beamforming algorithms but also to ESPRIT algorithm. All the predicted results are verified by
simulations.

This work was supported in part by the NSF grant MIP-93-09-506, the ONR grant
N00014-93-1-0566, and MIPS/Watkins Johnson.
I Introduction

Sensor array processing has been a key technology in radar, sonar, communications and biomedical signal processing. Recently, as the cellular communication technology advances, sensor array processing emerges as a potential technology to improve the spectral efficiency [1], [2], [3].

Much of the work in array processing has focused on methods for high-resolution DOA estimation and optimum adaptive beamforming. These methods include the well known MUSIC [4] algorithm and ESPRIT [5] algorithm for DOA estimation and MVDR and LCMV algorithms [6], [7], [8] for beamforming. However, an important drawback of these techniques is the severe degradation of the estimation accuracy in DOA estimation [9] or signal cancellation [10] in adaptive beamforming, in the presence of highly correlated or coherent signals.

To counter the deleterious effects due to some coherent signals, a pre-processing scheme referred to as spatial smoothing (SS) proposed by Evans et al. [11] and further developed by Shan et al. [9], [12] has been shown to be effective in decorrelating coherent signals. However, such a scheme is only applied to uniformly spaced linear arrays. Linear arrays are known to be limited to estimating azimuth angles within 180°, and practically effective only for signals from broadside direction. The degree of SS using a uniformly spaced linear array is also sensitive to DOA’s [13]. As a result, a linear array is not very effective in radar, sonar, or especially in cellular communications where users can never predict the incoming directions of the moving targets.

In the past decade, research has been carried out in developing algorithms for coherent interference using arrays of arbitrary geometry. In the area of DOA estimation, multidimensional subspace fitting algorithms such as deterministic maximum likelihood (DML) [14], multidimensional (MD)-MUSIC [15], and recently proposed weighted subspace fitting (WSF) [16], [17], are effective in both coherent and noncoherent environment and can be applied to arrays of arbitrary geometry. However, all these algorithms involve some searching procedures used to solve nonlinear equations. They are computationally intensive and are not practical in real-time applications. Several other techniques map the signal received by the array to a virtual array, but these methods all need approximations and have restricted applications. In the area of narrow-band adaptive beamforming, The coherent interference suppression using null constraint with an array of arbitrary geometry was addressed in [18]. This approach still requires pre-estimation of arrival angles of coherent interferences. The SPT-LCMV beamforming algorithm applicable to arrays of arbitrary geometry was considered in [19]. This algorithm requires increased computational complexity.
compared to LCMV. Recently, diversity combining [21] and blind adaptive beamforming [20] have been proposed to combat multipath fading and cochannel interference. However, blind adaptive beamformer has a low convergence rate, and is only applied to signals with constant modulation. Both techniques have limitations on tracking complicated channels while cochannel interference and multipath effects coexist.

In this work, we develop a general SS technique for arrays of arbitrary geometry to make MUSIC, ESPRIT algorithms and optimum adaptive beamforming algorithms operative in a coherent interference environment and meanwhile achieve robustness in performance. Compared with the aforementioned methods for arrays of arbitrary geometry, this SS technique can be easily implemented. It does not increase the computational complexity of either MUSIC, ESPRIT, or adaptive beamforming. It allows us to work on a data domain [22], and thus enables us to incorporate the recently developed URV [23] [24] algorithm to DOA estimation and updating and enables us to implement MVDR beamforming algorithm using systolic arrays. Therefore it has great potential in mobile radio communication where coherent and cochannel multipath interference is a major problem. Also, it can be used in conjunction with MUSIC or ESPRIT algorithm to provide an initialization for the WSF method to get a more accurate DOA estimation [17].

Specifically, we discovered and proved the necessary and sufficient conditions on an array geometry for applying SS. They are: (1) such an array must have an orientational invariance structure; (2) its center array has an ambiguity free array manifold; and (3) the number of subarrays is larger than or equal to the largest number of mutually coherent signals. By working on a smoothed data matrix obtained from SS, we can use MUSIC and optimum adaptive beamformers effectively in a coherent interference environment. To further increase efficiency and estimation resolution, we found that the forward/backward spatial smoothing [25] (FBSS), when applied to a nonlinear array of central symmetry, can reduce the number of sensors required and improve the estimation resolution for closely spaced incoming signals. Finally we expand the application of our results to ESPRIT.

In all the papers cited above that dealt with DOA estimation with arrays of arbitrary geometry, ambiguity free array manifolds were assumed. In [4] Schmidt discovered and defined the rank-$n$ ambiguity in an array manifold. In [28], Lo and Marple proved the conditions for a rank-2 ambiguity. In [26] ambiguities of linear arrays were studied. However, constructing an nonlinear array free of up to rank-$k$ ambiguities using only $(k + 1)$ sensors remains a challenging problem [27]. In this paper, we report a more thorough study on this issue. We proved the necessary and sufficient conditions
for a three-sensor array manifold to be ambiguity free. We then identified several situations, for higher order sensor array manifolds, in which ambiguity may arise. Thus we get corresponding necessary conditions to design ambiguity free center arrays and subarrays.

This paper is divided into six sections. In section II, we prove the necessary and sufficient conditions on an array of nonlinear geometry for applying SS, and consider the FBSS technique for applications in nonlinear arrays. In section III, we study the cause of ambiguities in a multipath signal environment. In section IV, we present some practical considerations and simulation results. In section V, we expand our results to ESPRIT. Section VI concludes our work.

II SS for Array of Arbitrary Geometry

We first assume that all the sensors in an array discussed in this paper are omnidirectional and identical. Consider an array of $p$ sensors. Let $d$ narrow-band signals with additive white Gaussian noise impinge on the array at incident angles $\theta_1, \cdots, \theta_d$. The array output covariance matrix has the form [22]

$$R = E(r(t)r^H(t)) = AR_sA^H + \sigma^2 I,$$

where $r(t)$ is the received signal vector by the array at time $t$, $A$ is a $p \times d$ steering matrix and $\sigma^2$ is the variance of the white Gaussian noise. When there are coherent interferences, the signal covariance matrix $R_s$ is no longer full rank. Therefore, all the high resolution DOA estimation methods based on eigendecomposition and all the adaptive beamforming algorithms which assume that interfering signals are not fully correlated with the desired signals fail to operate effectively.

In the case of a uniformly spaced linear array, with a sensor spacing $\Delta$, the SS algorithm [9] [12] can be applied to achieve the nonsingularity of the modified covariance matrix of the signals. This technique begins by dividing a uniformly spaced linear array of $L$ sensors into $K$ overlapping subarrays of size $p$, with sensors $\{1, \cdots, p\}$ forming the first subarray, and sensors $\{2, \cdots, p + 1\}$ forming the second subarray, etc. It was shown that [9]

$$A_k = A_1E^{(k-1)},$$

where $A_k$, $k = 1, \cdots, K$, is a $p \times d$ steering matrix consisting of steering vectors associated with the $k$th subarray, and $E^{(k)}$ denotes the $k$th power of a $d \times d$ diagonal matrix $E$. 

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The spatially smoothed covariance matrix is defined as the average of the subarray covariances:

$$\tilde{R} = \frac{1}{K} \sum_{k=1}^{K} R_k = A_1 \tilde{R}_s A_1^H + \sigma^2 I, \quad (3)$$

where $R_k$ is the covariance matrix associated with the $k$th subarray, $\tilde{R}_s$ is the modified covariance matrix of the signals, and has been proved [9] to be full rank when $K \geq d$. The signals are thus progressively decorrelated [13]. However, linear arrays have limitations in the domain of estimable DOA’s. It has been shown in [29] that $\tilde{R}_s$ can be decomposed as follows:

$$\tilde{R}_s = \frac{1}{K} C C^H \quad (4)$$

where $C = P A^T$ with $P = \text{diag}(p_1, p_2, \cdots, p_d)$, and

$$A = \begin{bmatrix}
1 & 1 & \cdots & 1 \\
\frac{-j2\pi}{\Delta} \sin(\theta_1) & \frac{-j2\pi}{\Delta} \sin(\theta_2) & \cdots & \frac{-j2\pi}{\Delta} \sin(\theta_d) \\
\frac{-j4\pi}{\Delta} \sin(\theta_1) & \frac{-j4\pi}{\Delta} \sin(\theta_2) & \cdots & \frac{-j4\pi}{\Delta} \sin(\theta_d) \\
\vdots & \vdots & \ddots & \vdots \\
\frac{-j2K\pi}{\Delta} \sin(\theta_1) & \frac{-j2K\pi}{\Delta} \sin(\theta_2) & \cdots & \frac{-j2K\pi}{\Delta} \sin(\theta_d)
\end{bmatrix}. \quad (5)$$

When incoming signals are closely spaced, the columns of both $A$ and $A_1$ become almost linearly dependent [29]. The dependency increases drastically when some of $\sin(\theta_i), i = 1, \cdots, d$ approach 1 for DOA’s near $90^0$. As a result, the performance of a linear array deteriorates quickly when some of DOA’s approach $90^0$. The highly directional sensitivity of the linear array causes the lack of performance robustness to the DOA’s and limits the domain of estimable angles to azimuth angles from broadside direction of the array. The lack of performance robustness of a linear array is even more severe when SS technique is applied, because in the smoothed covariance matrix, not only the steering matrix $A_1$, but also $A$ is ill-conditioned in the situation described above. A general SS technique that is robust and can be applied to directionally independent arrays is thus more desirable.

## A Orientational Invariance Structure

It is apparent that the mapping relation between $A_k$ and $A_1$ is the key to successful application of the SS technique. In general, we can divide an arbitrary array into $K$ subarrays which may overlap.
There is not always a steering matrix $A$ to map all the steering matrix $A_k$, for $k = 1, \cdots, K$ to $A$. In this section, we will develop necessary and sufficient conditions on array geometries for implementing the general SS. First, we give the following lemmas.

**Lemma 1** For steering matrices $A$ and $B$, given by $A = [a(0_1), \cdots, a(0_d)]$ and $B = [b(0_1), \cdots, b(0_d)]$, there exists a mapping relation $B = AC$ if and only if $C$ is a diagonal matrix.

**Lemma 2** For $K$ steering matrices $A_1, A_2, \cdots, A_K$, each $A_i$ can be mapped to a steering matrix $B$ if and only if there exists a mapping relation $A_j = A_iC_{ij}$ for any $i$ and $j$.

The proofs of both lemmas are given in the Appendix.

Consider an array that is divided into $K$ subarrays. Suppose $A_i$ and $A_j$ are the steering matrices associated with the $i$th and the $j$th subarrays, and there are $d$ signals with incoming angles $\theta_1, \cdots, \theta_d$. $A_i$ can be written as

$$A_i = [a_i(0_1), a_i(0_2), \cdots, a_i(0_d)], \tag{6}$$

where $a_i^T(0_k) = [e^{-j\phi_{i1}(0_k)}, e^{-j\phi_{i2}(0_k)}, \cdots, e^{-j\phi_{ip}(0_k)}], k = 1, \cdots, d$, is the steering vector associated with the $i$th subarray, and $\phi_{il}(0_k), l \in \{1, \cdots, p\}$, is the phase delay of the $k$th signal at the $l$th sensor of the $i$th subarray from the first sensor of the first subarray. We refer to the sensor of an array associated with the $l$th row of a steering matrix of the array as the $l$th sensor of the array.

Let $\Delta_{ijl}, 1 \leq l \leq p$, represent the distance between the $l$th sensor in the $i$th subarray and the $l$th sensor in the $j$th subarray. Let $\beta_{ijl}$ represent the angle of the line on which these two sensors are located. If the $i$th and the $j$th subarrays are identical and have the same orientation, i.e. all $\Delta_{ijl}$ for $l = 1, \cdots, p$ are equal and all $\beta_{ijl}, l = 1, \cdots, p$ are equal, then the phase delay of a signal with an incoming angle $\theta_k$ from each sensor in the $i$th subarray to the corresponding sensor in the $j$th subarray is the same according to the far field assumption. We denote this phase delay by $\Phi_{ij}(0_k)$. For any $l \in \{1, \cdots, p\}$, we have

$$\Phi_{ij}(0_k) = \phi_{jl}(0_k) - \phi_{il}(0_k) = 2\pi \frac{\Delta_{ijl}}{\lambda} \sin(\beta_{ijl} - \theta_k + \frac{\pi}{2}), \tag{7}$$

then $A_j = A_iC_{ij}$, where $C_{ij}$ is a diagonal matrix with the $m$th diagonal element $e^{-j\Phi_{ij}(0_m)}$. The identical and orientational invariance properties between two subarrays guarantee a mapping relation between their steering matrices.
On the other hand, if \( A_j = A_i C \), by Lemma 1, \( C \) should be a diagonal matrix and can be represented by \( C = \text{diag}\{c_{11}(\theta_1), c_{22}(\theta_2), \cdots, c_{dd}(\theta_d)\} \). It requires that
\[
e^{-j\phi_{il}(\theta_k)} c_{kk}(\theta_k) = e^{-j\phi_{jl}(\theta_k)} \quad \text{for} \quad l = 1, \cdots, p,
\] (8)
which can be simplified to
\[
\phi_{jl}(\theta_k) - \phi_{il}(\theta_k) = \Phi_{ij}^\prime(\theta_k) + 2\pi n, \quad \text{for} \quad l = 1, \cdots, p
\] (9)
where \( n \) can be any integer. The relation in (9) holds for all \( \theta_k \) in \([0, 360)\) only if \( \Delta_{ij1} = \Delta_{ij2} = \cdots = \Delta_{ijp} \) and \( \beta_{ij1} = \beta_{ij2} = \cdots = \beta_{ijp} \), i.e. the \( i \)th and the \( j \)th subarrays must be identical and have the same orientation. Thus, we have Lemma 3:

**Lemma 3** Suppose \( A_i \) and \( A_j \) are steering matrices associated with the \( i \)th and the \( j \)th subarrays. The sensors in each subarray are numbered in the same sequence. There exists a mapping relation \( A_j = A_i C_{ij} \) if and only if the \( i \)th and the \( j \)th subarrays are identical and have the same orientation.

From Lemmas 2 and 3, we have:

**Theorem 1** Suppose an array can be divided into \( K \) subarrays, each having a \( p \times d \) steering matrix \( A_i, i = 1, 2, \cdots, K \). All \( A_1, A_2, \cdots, A_K \) can be mapped to a \( p \times d \) steering matrix \( B \) by \( A_i = BD_i \) if and only if all these subarrays are identical and have the same orientation.

We call the array structure held by an array satisfying conditions in Theorem 1 the orientational invariance structure. A more rigorous definition is given as follows:

**Definition 1 (Orientational Invariance Structure)** An array has an orientational invariance structure if it can be divided into subarrays that are identical and have the same orientation.

For an array with orientational invariance structure, we can consider each subarray as one element located at its first sensor. Then all these elements form a center array. A more rigorous definition for center array is given as follows:

**Definition 2 (Center Array)** If an array with orientational invariance structure is divided into subarrays (which can have overlap), then the collection of all the first sensors of these subarrays form a center array.
B Necessary and Sufficient Conditions

Suppose an array has an orientational invariance structure. Moreover, its center array has an ambiguity free structure and the number of subarrays is larger than or equal to the largest number of mutually coherent signals. The \( p \times d \) steering matrices \( A_1, A_2, \cdots, A_K \) are associated with the subarrays \( 1, 2, \cdots, K \), respectively, and \( d_k \) is the distance between the first sensor in the first subarray and the first sensor in the \( k \)th subarray. The angle \( \beta_k \) represents the direction of the line on which the first sensor in the first subarray and the first sensor in the \( k \)th subarray are located (see Fig.1). We have

\[
A_k = A_1 D_k, \quad k = 2, \cdots, K
\]

where

\[
D_k = \begin{bmatrix}
e^{-j \frac{2\pi d_k}{\lambda} \sin(\beta_k - \theta_1 + \frac{\pi}{2})} \\
e^{-j \frac{2\pi d_k}{\lambda} \sin(\beta_k - \theta_2 + \frac{\pi}{2})} \\
\vdots \\
e^{-j \frac{2\pi d_k}{\lambda} \sin(\beta_k - \theta_d + \frac{\pi}{2})}
\end{bmatrix}
\]

The covariance matrix of the \( k \)th subarray is thus given by

\[
R_k = A_1 D_k R_s D_k^H A_1^H + \sigma^2 I,
\]

where \( R_s \) is the covariance matrix of the source. The spatially smoothed covariance matrix is defined as the average of the subarray covariances

\[
\bar{R} = \frac{1}{K} \sum_{k=1}^{K} R_k = A_1 \bar{R}_s A_1 + \sigma^2 I,
\]

where \( \bar{R}_s \) is the modified covariance matrix of the signal given by

\[
\bar{R}_s = \frac{1}{K} \sum_{k=1}^{K} D_k R_s D_k^H.
\]

We will show in the following that \( \bar{R}_s \) is nonsingular. First, \( \bar{R}_s \) can be written as
\[
\tilde{R}_s = [I \hspace{1cm} D_2 \hspace{1cm} \cdots \hspace{1cm} D_K] \begin{bmatrix}
\frac{1}{K} R_s \\
\frac{1}{K} R_s \\
\vdots \\
\frac{1}{K} R_s \\
\end{bmatrix} \begin{bmatrix}
I \\
D_2^H \\
\vdots \\
D_K^H \\
\end{bmatrix}.
\]

Let \( C \) denote the Hermitian square root of \( \frac{1}{K} R_s \), i.e.

\[
CC^H = \frac{1}{K} R_s.
\]

It follows that

\[
\tilde{R}_s = GG^H
\]

where \( G \) is a \( d \times Kd \) block matrix given by

\[
G = [C \hspace{1cm} D_2 C \hspace{1cm} \cdots \hspace{1cm} D_K C].
\]

Clearly, the rank of \( \tilde{R}_s \) is equal to the rank of \( G \). Suppose there are \( q \) groups of signals in \( d \) incoming signals, with \( l_i, i = 1, \cdots, q \), correlated signals in each group. \( R_s \) must be a block diagonal matrix with block size \( l_i, i = 1, \cdots, q \). We can thus get a corresponding block diagonal matrix \( C \). Recall that the rank of a matrix is unchanged after a change of its columns. By grouping columns of similar elements, we can verify that

\[
\rho(G) = \rho
\begin{bmatrix}
\begin{array}{cccc}
\vdots & \cdots & \cdots & \vdots \\
\vdots & c_{1_1,1_1} b_1 & \cdots & c_{1_1,l_1} b_1 \\
\vdots & \cdots & \cdots & \vdots \\
\vdots & c_{1_1,1_1} b_{l_1} & \cdots & c_{1_1,l_1} b_{l_1} \\
\vdots & \cdots & \cdots & \vdots \\
\vdots & \cdots & \cdots & \vdots \\
\vdots & c_{d_1-l_1+1,d_1-l_1+1} b_{d_1-l_1+1} & \cdots & c_{d_1-l_1+1,d_1} b_{d_1-l_1+1} \\
\vdots & \cdots & \cdots & \vdots \\
\vdots & \cdots & \cdots & \vdots \\
\cdots & \cdots & \cdots & \cdots \\
\cdots & \cdots & \cdots & \cdots \\
\cdots & \cdots & \cdots & \cdots \\
\cdots & \cdots & \cdots & \cdots \\
\cdots & \cdots & \cdots & \cdots \\
\cdots & \cdots & \cdots & \cdots \\
\cdots & \cdots & \cdots & \cdots \\
\cdots & \cdots & \cdots & \cdots \\
\cdots & \cdots & \cdots & \cdots \\
\end{array}
\end{bmatrix}
\]

where \( \rho \) is a rank operator, \( c_{ij} \) is the \( ij \)th element of matrix \( C \), and \( b_i (i = 1, \cdots, d) \) is the \( 1 \times K \) row vector given by

\[
b_i = [1 \hspace{1cm} e^{-j \frac{2\pi d_2}{\lambda} \sin(\theta_2-\theta_i+\frac{\pi}{2})} \hspace{1cm} e^{-j \frac{2\pi d_3}{\lambda} \sin(\theta_3-\theta_i+\frac{\pi}{2})} \hspace{1cm} \cdots \hspace{1cm} e^{-j \frac{2\pi d_K}{\lambda} \sin(\theta_K-\theta_i+\frac{\pi}{2})}].
\]
Each row of matrix \( C \) has at least one nonzero element because the energy of each signal is nonzero. It is observed that \( b_i \) is the transpose of the steering vector associated with the center array. Since the center array is assumed to have ambiguity free array manifold, when \( K \geq \max\{l_1, l_2, \cdots, l_q\} \), all the \( b \) vectors associated with all the signals within a group of coherent signals are thus linearly independent. Therefore, \( G \) is of full row rank and the modified covariance matrix \( \tilde{R}_S \) is of full rank. Otherwise, if \( K < \max\{l_1, l_2, \cdots, l_q\} \), we will see that \( \tilde{R}_s \) is rank deficient. We assume that \( R_{si} \) is the correlation matrix associated with the \( i \)th group of coherent signals. Thus, \( R_{si} \) has rank 1 and can be expressed as \( \lambda_i h_i h_i^H \) where \( \lambda_i \) and \( h_i \) are the corresponding eigenvalue and eigenvector of \( R_{si} \). We have

\[
R_s = \begin{bmatrix}
R_{s1} & & & \\
 & R_{s2} & & \\
& & \ddots & \\
& & & R_{sq}
\end{bmatrix} = \begin{bmatrix}
\lambda_1 h_1 h_1^H & & & \\
& \lambda_2 h_2 h_2^H & & \\
& & \ddots & \\
& & & \lambda_q h_q h_q^H
\end{bmatrix}
\] (21)

and

\[
\tilde{R}_s = \begin{bmatrix}
\sum_{k=1}^{K} \lambda_1 (D_{k1} h_1)(D_{k1} h_1)^H \\
& \sum_{k=1}^{K} \lambda_2 (D_{k2} h_2)(D_{k2} h_2)^H \\
& & \ddots \\
& & & \sum_{k=1}^{K} \lambda_q (D_{kq} h_q)(D_{kq} h_q)^H
\end{bmatrix}
\] (22)

where \( D_{ki} \) is a diagonal matrix consisting of \( l_i \) diagonal elements of \( D_k \) which are associated with all the DOA's from \( i \)th group of coherent signals. Since

\[
\rho(\sum_{k=1}^{K} \lambda_i (D_{ki} h_i)(D_{ki} h_i)^H) \leq \min(K, l_i)
\] (23)

and

\[
\dim(\sum_{k=1}^{K} \lambda_i (D_{ki} h_i)(D_{ki} h_i)^H) = l_i \times l_i,
\] (24)

thus \( \tilde{R}_s \) is rank deficient if \( K \leq \max(l_1, l_2, \cdots, l_q) \).

If the center array is not ambiguity free, then all the \( b \) vectors associated with all the signals within a group of coherent signals can be linearly dependent, \( G \) cannot be ensured to be of full row rank, and neither can \( R_s \).
From Theorem 1 and the proof above, we get the following theorem.

**Theorem 2** SS can be applied to an array of arbitrary geometry to obtain a full rank smoothed signal covariance matrix if and only if an array has an orientational invariance structure, its center array has an ambiguity free structure, and the number of subarrays is larger than or equal to the size of the largest group of coherent signals.

C  Further Improvement

To get a smoothed nonsingular covariance matrix \( \hat{R}_s \) by using the SS technique, we need \( K \geq \max\{l_1, l_2, \cdots, l_q\} \). We can further reduce the number of subarrays by getting another \( K \) backward subarrays similar to the case in a linear array [25]. Although, the Forward-Backward Spatial Smoothing (FBSS) [25] can always be applied in a uniformly spaced linear array. For arrays of arbitrary geometry, there is some requirements on the geometry for successful implementation of the backward method. We first give the definition of central symmetry:

**Definition 3 (Central Symmetry)** The array is central symmetric if it is identical before and after rotating \( 180^\circ \) about its center of mass.

If an array is central symmetric, we can get \( K \) additional backward subarrays by reversing the order of the subarrays and the order of the sensors within each subarray.

Let \( r_k^r(t) \) denote the complex conjugate of the output of the \( k \)th backward subarray for \( k = 1, \cdots, K \). We have

\[
  r_k^r(t) = A_1 D_k (D_L s(t))^* + \mathbf{n}^*(t)  \tag{25}
\]

where \( \mathbf{n}(t) \) is an additive white Gaussian noise vector, \( D_L \) is a diagonal matrix with the \( i \)th diagonal element given by \( e^{-j2\pi \frac{d_{Kp}}{\lambda} \sin(\beta_{Kp} - \theta_i + \frac{\pi}{2})} \) and \( d_{Kp} \) is the distance between the first sensor in the first forward subarray and the first sensor in the first backward subarray. The angle \( \beta_{Kp} \) represents the direction of the line on which the two sensors are located.

The covariance matrix of the \( k \)th backward subarray is given by

\[
  R_k^b = A_1 D_k R_s^r D_k^H A_1^H + \sigma^2 I  \tag{26}
\]

with

\[
  R_s^r = E(D_L^* s^r(t) s^T(t) D_L^r) = D_L^* R_s^r D_L^r.  \tag{27}
\]
Define the spatially smoothed backward subarray covariance matrix \( \tilde{R}^b \) as the average of these subarray covariance matrices, i.e.,

\[
\tilde{R}^b = \frac{1}{K} \sum_{k=1}^{K} R_k^b = A_1 \tilde{R}_s A_1^H + \sigma^2 I, \tag{28}
\]

where

\[
\tilde{R}_s^b = \frac{1}{K} \sum_{k=1}^{K} D_k R_k^b D_k^H, \tag{29}
\]

and define the forward/backward smoothed covariance matrix \( \tilde{R} \) as the average of \( \tilde{R} \) in (13) and \( \tilde{R}^b \), i.e.,

\[
\tilde{R} = \frac{\tilde{R} + \tilde{R}^b}{2} = A_1 \tilde{R}_s A_1^H + \sigma^2 I. \tag{30}
\]

It follows that

\[
\tilde{R}_s = \frac{\tilde{R}_s + \tilde{R}_s^b}{2}. \tag{31}
\]

We can show, in a similar way as in the case of a linear array [25], that the modified source covariance matrix \( \tilde{R}_s \) is nonsingular as long as \( 2K \geq \max\{l_1, l_2, \ldots, l_q\} \).

### III Ambiguity Free Array Structure

To perform SS, we need an ambiguity free center array manifold. Also, to perform MUSIC, we further require ambiguity free subarray manifolds. Ambiguity arises when a steering vector can be expressed as a linear combination of other steering vectors in an array manifold [4]. For a uniformly spaced linear array, rank-1 ambiguity [4] cannot be avoided since the DOA's which are "mirror images" with respect to the array line, have the same steering vector. This limits the range of DOA's estimable by a uniformly spaced linear array to within 180°. Suppose an array has \( p \) elements, then rank-\( p \) [4] ambiguities cannot be avoided. In this paper, an ambiguity free array manifold of an array of \( p \) sensors refers to rank-(\( p-1 \)) ambiguity free. Generally, to avoid ambiguity, an array used for high-resolution DOA estimation must have a proper structure. An ambiguity free array manifold has been assumed in several papers [5], [17], [15]. Our attempt is to identify all the situations in which ambiguity may arise. One of our guidelines in designing arrays is to avoid these identified ambiguities.
Theorem 3 In an azimuth only system, the necessary and sufficient condition for an ambiguity free three-sensor array manifold is that all these three sensors are not on one line and that the distance between any two sensors is less than or equal to $\frac{\lambda}{2}$.

The proof is given in the appendix.

We can see in general that (a) rank-1 ambiguity occurs not only in uniformly spaced linear arrays but also in rectangular arrays with sensors having a uniform spacing of $\frac{\lambda}{2}$ along either x-axis or y-axis, (b) rank-2 ambiguity occurs in an array that consists of two parallelly positioned linear arrays with an identical uniform sensor spacing that is larger than $\frac{\lambda}{2}$, (c) rank-3 ambiguity occurs in an array that consists of three parallelly positioned linear arrays with an identical uniform sensors spacing that is larger than $\frac{\lambda}{2}$, and (d) higher order ambiguity occurs if more than $\lfloor \frac{k}{2} \rfloor$ sensors are on one line in a $k$ sensor array or if an array consists of $m$ parallelly positioned linear arrays with an identical uniform sensor spacing that is larger than $\frac{\lambda}{2} \lfloor \frac{m}{2} \rfloor$. These situations are shown schematically in Fig.3(a)-(d). In Fig.3 (b) and (c), the angles $\theta$ and $\alpha$ satisfy the following constraint:

$$2\pi \frac{d}{\lambda} \sin(\alpha) + 2k\pi = 2\pi \frac{d}{\lambda} \sin(\theta), \quad k \in \{1, 2, \ldots\}.$$  \hfill (32)

In Fig.3 (d), the angles $\theta$, $\beta$ and $\alpha$ satisfy the following constraint:

$$2\pi \frac{d}{\lambda} \sin(\alpha) + 2k_1\pi = 2\pi \frac{d}{\lambda} \sin(\beta) + 2k_2\pi = 2\pi \frac{d}{\lambda} \sin(\theta),$$  \hfill (33)

where $k_1, k_2 \in \{1, 2, \ldots\}$ and $k_1 \neq k_2$.

To get an ambiguity free array manifold, it is necessary to avoid these identified situations.

IV Implementation and Simulation Results

A Some Practical Considerations

To determine the source coherency structure, we can use SRP [30]. On the other hand, we can estimate the maximum number of incoming angles according to the multipath environment. In this paper, limited by space, we assume the number of incoming signals is given.

In practice, we can perform FBSS by setting up a special data matrix. Specifically, for the $n$th
snapshot we set up the data matrix

\[ A^H(n) = \begin{bmatrix}
  u(p,1,n) & \cdots & u(p,K,n) & u^*(1,K,n) & \cdots & u^*(1,1,n) \\
  u(p-1,1,n) & \cdots & u(p-1,K,n) & u^*(2,K,n) & \cdots & u^*(2,1,n) \\
  \vdots & \ddots & \vdots & \vdots & \ddots & \vdots \\
  u(1,1,n) & \cdots & u(1,K,n) & u^*(p,K,n) & \cdots & u^*(p,1,n)
\end{bmatrix} \] (34)

where \( u(i,j,n) \) denotes the sample taken at the \( i \)th sensor of the \( j \)th subarray. For the totality of \( N \) snapshots, we can define the overall data matrix

\[ A^H = \begin{bmatrix} A^H(1), A^H(2), \cdots, A^H(N) \end{bmatrix}. \] (35)

It follows that the averaged smoothed correlation matrix \( \tilde{R} \) (as defined in (30)) can be estimated as follows:

\[ \tilde{R} = \frac{1}{2NK} A^HA. \] (36)

As we know, more robust results can be obtained from data domain rather than from covariance domain [22]. We can proceed with MUSIC [22] algorithm or MVDR [7] [22] beamforming algorithm based on \( \tilde{A} \) instead of \( \tilde{R} \).

An array needs to be chosen for applying SS. Such an array should satisfy all conditions aforementioned. An omnidirectional circular array has been a conventional choice for mobile communications [1] [2], and there have been active research efforts to find a pre-processing scheme for the circular array to handle the coherent interference [31]. However, we can see clearly from our discussion that a single circular array is not orientational invariant. Therefore it does not satisfy the necessary condition for applying SS. This implies that the circular array cannot overcome the coherent interference by using the SS technique. For some circular arrays with central symmetric, we can apply FBSS to handle two coherent signals. To handle more than two coherent signals, several parallelly positioned circular arrays have to be used.

B Selecting Orientational Invariance Structure

In this section, we study some guidelines for designing an optimal sensor array for SS. We found that the sensor utilization rate is an important factor for estimating DOA’s of coherent signals with SS.
Definition 4 (Sensor Utilization Rate (SUR))

\[ SUR = \frac{\sum n_{\text{subarray}}}{n_{\text{array}}} \]  

(37)

where \( \sum n_{\text{subarray}} \) is the sum of the number of sensors in each subarray, and \( n_{\text{array}} \) is the total number of sensors in the whole array. Obviously \( SUR \geq 1 \), because of possible overlap of subarrays.

Example 1: We perform simulations on two 64-element arrays: (1) a hollow square array as shown in Fig.4(a), which has a low SUR for a given number of sensors, and (2) a dense square array, as shown in Fig.4(b), which has a high SUR. The dense square array contains 4 subarrays each having 49 sensors. The spacing between two neighboring sensors is 0.45\( \lambda \). The SUR of the array is approximately 3. The hollow square array contains 4 subarrays, each having 32 sensors. The spacing between two neighboring sensors is 0.45\( \lambda \). The SUR is 2. Both structures are used to estimate the DOA’s of two coherent signals. The input SNR is 20dB. We use the FBSS method. The simulation results are shown in Fig.5. In cases (a) and (b), the two coherent signals are at 40° and 50°. Both arrays can clearly identify the DOA’s. In cases (c) and (d), the two coherent signals are at 45° and 50°, only the dense square array can determine the DOA’s. Our results show that a dense square array structure is better than a hollow square array structure.

For a uniformly spaced linear array, the larger the physical aperture, the narrower the beamwidth, and the higher the resolution. For a nonlinear array, the DOA resolution is however decided by an effective array beamwidth. The beamwidth \( b_{1,2} \) of two signals, with DOA at \( \theta_1 \) and \( \theta_2 \), arriving at an array with steering vector \( \mathbf{v}(\theta) \) is evaluated by the following equation.

\[ b_{1,2} = \frac{2}{\pi \cos^{-1}(\frac{\mathbf{v}^H(\theta_1)\mathbf{v}(\theta_2)}{||\mathbf{v}(\theta_1)|| ||\mathbf{v}(\theta_2)||})} \]  

(38)

We compared the beamwidths between a dense square subarray and a hollow square subarray. In Fig. 6, we plot the beamwidths of two signals, that are 10° and 5° apart in (a) and (b), respectively, versus the angle of arrival of the signal that has a smaller DOA values. We see that although the dense square array has a smaller physical array aperture, it has a narrower beamwidth. Since both arrays have the same number of elements, we infer that SUR is an important factor and needs to be maximized in the array design. An array consisting of several parallely positioned circular arrays has a low SUR and is not recommended for SS applications.
C Simulation Results

In this section, we present some simulation results on MUSIC algorithm to show the effectiveness and applications of our SS and FBSS. We choose a square array, which has an orientational invariance structure, central symmetric, and a sensor spacing less than $\frac{1}{2}$.

**Example 2:** To compare the performance of a square array to that of a linear array under the same complexity, we use a nine-sensor linear array and a nine-sensor square array as shown in Fig.7, both having a spacing of $0.45\lambda$ between neighboring sensors. We divide the both arrays into four overlapped subarrays. We get six and four sensors in each subarray of the linear array and the square array respectively. The resolution of DOA estimations is decided by the beamwidth of the subarrays. We consider two narrow-band coherent signals with DOA's at $70^\circ$ and $85^\circ$. The SNR is 20 dB. A total of 500 samples ("snapshots") are taken from the array. We use SS as a pre-processing scheme for MUSIC. Fig.8 shows that the DOA's of the two coherent signals are not resolved using a linear array, whereas the square array gives a satisfactory result. In Fig. 9, we plot the beamwidths of two signals, that are $15^\circ$ apart, versus the angle of arrival of the signal that has a smaller DOA values. For the linear array, actual beamwidth varies greatly with the DOA. The square array, however, shows a relatively stable beamwidth for different DOA's. When DOA's are at $70^\circ$ and $85^\circ$, the square array provides a narrower beamwidth and a higher resolution.

**Example 3:** We use the square array shown in Fig.7 to receive two coherent signals with DOA's at $75^\circ$ and $100^\circ$. We apply SS and FBSS separately. Fig.10 shows that the DOA estimation resolution achieved by a central symmetric array is significantly improved by using the FBSS method.

**Example 4:** In a wireless fading channel, coherent signals can not be avoided. Fig. 11 shows a typical example of the distribution of scatters in a mobile radio environment [33]. We can treat all the reflected signals from local scatterers as coming from a super position. However, those reflected signals from far away scatterers such as high rise buildings or mountains are all coherent signals. We use a dense square array of sixty-four sensors as shown in Fig.4(b) as the base station antenna. The array contains 4 subarrays each of 49 sensors. The spacing between two neighboring sensors is $0.45\lambda$. The array receives signals from four mobile users: four coherent signals at $20^\circ, 65^\circ, 150^\circ$ and $200^\circ$ from user 1, three at $230^\circ, 250^\circ$ and $280^\circ$ from user 2, two at $30^\circ$ and $300^\circ$ from user 3 and one at $320^\circ$ from user 4. The SNR is 20 dB. A total of 500 samples are used. First, we apply FBSS and then apply MUSIC. Simulation results are shown in Fig.12. According to these
DOA's information, we can further perform constrained beamforming and thus can achieve Spatial Division Multiple Access (SDMA) \cite{34} in a multipath environment.

We found the results obtained for a nonlinear array in an azimuth-only system remain valid in an azimuth-elevation system. The following is an example.

**Example 5:** We use the square array shown in Fig.7 to receive two coherent signals, one is at an azimuth of 40° and an elevation of 30°, and the other is at an azimuth of 50° and an elevation of 60°. The SNR is 20dB. The number of samples taken is 500. By using FBSS and MUSIC, we obtain the result in Fig.13. It demonstrates that a planar array enables us to perform DOA's estimation in a 3D domain while a linear array is not capable of doing that.

V Spatial Smoothing for ESPRIT

Similar to MUSIC, the ESPRIT algorithm \cite{5} is an approach to signal parameter estimation. It exploits an underlying data model at significant computational savings. The ESPRIT algorithm is also limited to estimating parameters in noncoherent incoming signals. The conventional SS can be incorporated into ESPRIT \cite{32}, but it requires the center array to be a uniformly spaced linear array. In this section, we show that our scheme also works for the ESPRIT algorithm to estimate parameters in a coherent interference environment.

In the ESPRIT algorithm, we consider \( d \) narrow-band plane waves with incident angles \( \theta_1, \cdots, \theta_d \), and wavelength \( \lambda \), impinge on a planar array of \( m \) sensors \( (m \text{ is even}) \), arranged in \( \frac{m}{2} \) doublet pairs. The displacement vector is the same for each doublet pair, but the location of each pair is arbitrary. The sensor output \( x(t) \) is given by

\[
x(t) = \begin{pmatrix} A \\ A\Phi \end{pmatrix} s(t) + n(t)
\]

(39)

where \( n(t) \) is a white Gaussian noise vector. \( A \) and \( A\Phi \) are the steering matrices corresponding to the first sensors and the second sensors in all pairs, respectively. The matrix \( \Phi \) is a diagonal \( d \times d \) matrix of phase delays between the doublet sensors for the \( d \) signals. The sensor output covariance matrix \( R_x \) is thus measured by

\[
R_x = \begin{pmatrix} A \\ A\Phi \end{pmatrix} R_s \begin{pmatrix} A \\ A\Phi \end{pmatrix}^H + \sigma^2 I.
\]

(40)
A full rank matrix $R_s$ is assumed when the ESPRIT algorithm is performed. If some of the incoming signals are coherent, $R_s$ will not be a full rank matrix and the ESPRIT will fail. The spatial smoothing technique we introduced in the previous sections can then be applied here to get a modified full rank signal covariance matrix.

We consider each doublet sensor pair in the array used by ESPRIT algorithm as one element. Then the array consists of $\frac{m}{2}$ elements. If this array has an orientational invariance structure with $K$ subarrays and the corresponding center array has an ambiguity free structure, the sensor output at the $k$th subarray is given by

$$x_k(t) = \begin{pmatrix} A_1 \\ A_1 \Phi \end{pmatrix} D_k s(t) + n(t).$$

(41)

Matrix $D_k$ is a diagonal $d \times d$ matrix of the phase delays in the form given in (11). The corresponding covariance matrix $R_{x_k}$ is given by

$$R_{x_k} = \begin{pmatrix} A_1 \\ A_1 \Phi \end{pmatrix} D_k R_s D_k^H \begin{pmatrix} A_1 \\ A_1 \Phi \end{pmatrix}^H + \sigma^2 I.$$

(42)

A smoothed output covariance matrix $\tilde{R}_x$ can thus be defined as

$$\tilde{R}_x = \frac{1}{K} \sum_{i=1}^{K} R_{x_k} = \begin{pmatrix} A_1 \\ A_1 \Phi \end{pmatrix} \tilde{R}_s \begin{pmatrix} A_1 \\ A_1 \Phi \end{pmatrix}^H + \sigma^2 I$$

(43)

where $\tilde{R}_s$ is the modified signal covariance matrix as defined in (14). As proved in Section II, $\tilde{R}_s$ is of full rank if $K$ is larger than or equal to the size of the largest group of coherent signals. We can now successfully perform ESPRIT based on $\tilde{R}_x$. We can also use FBSS to further reduce the number of sensors required and to improve the estimation resolution if the array of $\frac{m}{2}$ elements is central symmetric.

Although SS enables ESPRIT to estimate DOA's in a coherent interference environment, the estimation is still limited to identifying DOA's within $180^\circ$ in an azimuth only system. Hence, in terms of performance robustness to DOA's, our SS is more effective for MUSIC than for ESPRIT.

**Example 6:** A twelve sensor array shown in Fig.14 is used in this example to receive two coherent signals at $70^\circ$ and $80^\circ$. This array consists of two overlapping nine-sensor square arrays.
Each sensor in one square array and its counterpart in another form a doublet pair. These nine doublet pairs form an array which has orientational invariance structure and is central symmetric. The spacing between two neighboring sensors is 0.45\( \lambda \). The doublet spacing for ESPRIR is 0.45\( \lambda \). The SNR is 20dB. A total of 2000 trials are run. A histogram of the results is given in Fig.15. We apply FBSS first and then applied the ESPRIT. The two angles are clearly identified.

VI Conclusions

To significantly improve performance robustness in DOA estimation and in adaptive beamforming, we developed techniques for applying SS on arrays of nonlinear geometry, thus making MUSIC, ESPRIT and adaptive beamformers operative in a coherent interference environment. In order to apply SS to an array of nonlinear geometry, this array must have an orientational invariance structure and its center array must be ambiguity free. Also the number of subarrays must be greater than or equal to the largest number of mutually coherent signals. To apply SS in conjunction with MUSIC, all the subarrays must also be ambiguity free, and the number of sensors in each subarrays must be larger than the number of incoming signals. For ESPRIT, two identical arrays (or subarrays) separated by a displacement vector are used each satisfying the conditions for applying SS and MUSIC.

When a nonlinear array is central symmetric, the FBSS can be used and it outperforms the regular SS in terms of improved efficiency and estimation resolution.

We proved the necessary and sufficient conditions for a three-sensor array manifold to be ambiguity free. We identified several situations, for higher order sensor array manifolds, in which ambiguity may arise. It is necessary to avoid the identified ambiguities in designing ambiguity free center arrays and subarrays.

In practice, we found that we can choose a square array with a sensor spacing less than \( \frac{\lambda}{2} \) to meet all the conditions required for applying SS. Simulation results also show that for DOA estimation of coherent signals using SS, a square array has a preferred geometry in terms of the DOA estimation resolution and performance robustness.

VII Appendix

Proof of Lemma 1:
If part:

The proof is obvious and is omitted.

Only If part:

If $B = AC$, $A = [a(\theta_1), \cdots, a(\theta_d)]$ and $B = [b(\theta_1), \cdots, b(\theta_d)]$ and also assume $C$ is not a diagonal matrix, i.e. it has non-zero element $c_{lm}$ for $l \neq m$, then the steering vector $b(\theta_m)$ is

$$b(\theta_m) = \sum_{i=1}^{d} c_{im} a(\theta_i) = c_{im} a(\theta_l) + \sum_{i=1, i \neq l}^{d} c_{im} a(\theta_i). \quad (44)$$

This means that $b(\theta_m)$ is a function of variable $\theta_l$, which contradicts to the definition that $b(\theta_m)$ is only a function of $\theta_m$. Thus the assumption that $C$ is a non-diagonal matrix is false. $C$ has to be a diagonal matrix with $c_{ii} = \frac{b(\theta_i)}{a(\theta_i)}$.

Proof of Lemma 2:

If part:

Obviously, $B$ can be any of $\{A_1, A_2, \cdots, A_K\}$.

Only if part:

If each $A_i$ can be mapped to a steering matrix $B$, by definition there exist $C_i, C_j$ such that $A_i = B C_i, A_j = B C_j$. By Lemma 1, $C_i$ is a diagonal matrix. So $C_i^{-1}$ exists and is also a diagonal matrix. We have $A_j = A_i C_i^{-1} C_j$. Let $C_{ij} = C_i^{-1} C_j$, $C_{ij}$ is the product of two diagonal matrices. So $C_{ij}$ is also an diagonal matrix. $A_j = A_i C_{ij}$.

Proof of Theorem 3:

If part:

If sensors $A$, $B$ and $C$ are not on one line and their mutual distance is less than $\frac{\lambda}{2}$, without loss of generality, we let sensor $A$ be the first sensor in the array, $B$ the second and $C$ the third. The steering matrix of the array has the form

$$V = \begin{bmatrix} 1 & 1 & 1 \\ e^{j\phi_1(\theta_1)} & e^{j\phi_1(\theta_2)} & e^{j\phi_1(\theta_3)} \\ e^{j\phi_2(\theta_1)} & e^{j\phi_2(\theta_2)} & e^{j\phi_2(\theta_3)} \end{bmatrix} \quad (45)$$

where $\phi$ denotes phase delay. If the distance between any two sensors is $< \frac{\lambda}{2}$, the phase delay $\phi_1(\theta_i)$ and $\phi_2(\theta_i), i = 1, 2, 3$, are real numbers from $(-\pi, \pi)$.

Note that the steering matrix of the array corresponding to three incoming signals at different
angles is a special case of the general array in Lemma 2 of [28]. By Lemma 2 in [28], \( V \) is nonsingular with possible exception in one of the following three situations:

1. When \( \phi_1(\theta_1) = \phi_1(\theta_2) \), i.e. the two incoming signals are symmetric with respect to the line on which sensors \( A \) and \( B \) are located. Note that

\[
\det(V) = \begin{vmatrix}
0 & 1 & 0 \\
0 & 0 & 1 \\
& & \\
\end{vmatrix}
\]

\[
= \begin{vmatrix}
\cos(\phi_1(\theta_1)) - \cos(\phi_2(\theta_2)) & \cos(\phi_1(\theta_2)) - \cos(\phi_2(\theta_1)) \\
\cos(\phi_2(\theta_1)) - \cos(\phi_2(\theta_2)) & \cos(\phi_2(\theta_2)) - \cos(\phi_2(\theta_1)) \\
& & \\
\end{vmatrix}
\]

When \( \phi_1(\theta_1) = \phi_1(\theta_2) \), \( \det(V) = 0 \) if and only if \( \phi_2(\theta_1) = \phi_2(\theta_2) \) or \( \phi_1(\theta_3) = \phi_1(\theta_2) \). Since these sensors are not on one line, if \( \phi_1(\theta_1) = \phi_1(\theta_2) \), we have \( \phi_2(\theta_1) \neq \phi_2(\theta_2) \). Since \( \theta_1, \theta_2 \) and \( \theta_3 \) are three different angles, when \( \theta_1 \) and \( \theta_2 \) are symmetric with respect to the line, \( \theta_3 \) and \( \theta_2 \) can not be symmetric to the line, i.e. if \( \phi_1(\theta_1) = \phi_1(\theta_2) \), then we get \( \phi_1(\theta_3) \neq \phi_1(\theta_2) \). Thus, when \( \phi_1(\theta_1) = \phi_1(\theta_2) \), the matrix \( V \) is nonsingular.

2. Similarly, we can prove that when \( \phi_2(\theta_1) = \phi_2(\theta_2) \), the matrix \( V \) is nonsingular.

3. When \( \phi_1(\theta_1) - \phi_1(\theta_2) = \phi_2(\theta_1) - \phi_2(\theta_2) \), i.e. \( \phi_1(\theta_1) - \phi_2(\theta_1) = \phi_1(\theta_2) - \phi_2(\theta_2) \), \( \theta_1 \) and \( \theta_2 \) are symmetric with respect to the line connecting sensors \( B \) and \( C \). Note that

\[
\det(V) = \begin{vmatrix}
\cos(\phi_1(\theta_1)) - \cos(\phi_2(\theta_2)) & \cos(\phi_1(\theta_2)) - \cos(\phi_2(\theta_1)) \\
\cos(\phi_2(\theta_1)) - \cos(\phi_2(\theta_2)) & \cos(\phi_2(\theta_2)) - \cos(\phi_2(\theta_1)) \\
& & \\
\end{vmatrix}
\]

\[
= \begin{vmatrix}
\cos(\phi_1(\theta_1)) - \cos(\phi_2(\theta_2)) & \cos(\phi_1(\theta_2)) - \cos(\phi_2(\theta_1)) \\
\cos(\phi_2(\theta_1)) - \cos(\phi_2(\theta_2)) & \cos(\phi_2(\theta_2)) - \cos(\phi_2(\theta_1)) \\
& & \\
\end{vmatrix}
\]

When \( \phi_1(\theta_1) - \phi_2(\theta_1) = \phi_1(\theta_2) - \phi_2(\theta_2) \), \( \det(V) = 0 \) if and only if \( \cos(\phi_1(\theta_1)) = \cos(\phi_2(\theta_2)) \) or \( \cos(\phi_1(\theta_2)) = \cos(\phi_2(\theta_1)) \). Since the mutual distance between \( A, B \) and \( C \) are less than \( \frac{\pi}{2} \), \( \phi_2(\theta_1), \phi_2(\theta_2), \phi_1(\theta_2) - \phi_2(\theta_2) \) and \( \phi_1(\theta_3) - \phi_2(\theta_3) \) are all real numbers in \( (-\pi, \pi) \). \( \cos(\phi_1(\theta_1)) = \cos(\phi_2(\theta_2)) \) if and only if \( \phi_2(\theta_1) = \phi_2(\theta_2) \). \( \cos(\phi_1(\theta_2)) = \cos(\phi_2(\theta_1)) \) if and only if \( \phi_1(\theta_2) = \phi_2(\theta_2) \).

Since \( A, B \) and \( C \) are not on one line, if \( \theta_1 \) and \( \theta_2 \) are symmetric to the line connecting \( B \) and \( C \), they can not be symmetric to the line connecting \( A \) and \( B \) or \( A \) and \( C \). i.e., if \( \phi_1(\theta_1) - \phi_2(\theta_1) = \phi_1(\theta_2) - \phi_2(\theta_2) \), then \( \phi_1(\theta_3) - \phi_2(\theta_3) \neq \phi_1(\theta_2) - \phi_2(\theta_2) \). Thus, \( \phi_1(\theta_1) = \phi_1(\theta_2) \), the matrix \( V \) is nonsingular.
\( \phi_1(\theta_2) - \phi_2(\theta_2) \), we have \( \phi_2(\theta_1) \neq \phi_2(\theta_2) \). Since \( \theta_1, \theta_2 \) and \( \theta_3 \) are three different incoming angles, if \( \theta_1 \) and \( \theta_2 \) are symmetric to the line connecting \( B \) and \( C \), \( \theta_2 \) and \( \theta_3 \) can not be symmetric to the line, i.e., if \( \phi_1(\theta_1) - \phi_2(\theta_1) = \phi_1(\theta_2) - \phi_2(\theta_2) \), we have \( \phi_1(\theta_2) - \phi_2(\theta_2) \neq \phi_1(\theta_3) - \phi_2(\theta_3) \). Thus, when \( \phi_1(\theta_1) - \phi_2(\theta_1) = \phi_1(\theta_2) - \phi_2(\theta_2) \), the matrix \( V \) is nonsingular.

Therefore, we conclude that all the three situations which cause the singularity of the matrix in Lemma 2 of [28] will not cause the singularity of three-sensor steering matrix if three sensors are not on one line and their mutual distance is less than \( \frac{1}{2} \). Therefore the matrix \( V \) is full rank.

If the spacing between any two of the three sensors is not larger than \( \frac{1}{2} \), and there is at least one pair in these three sensors with a spacing of \( \frac{1}{2} \), then the only situation that the phase delay \( \phi_1(\theta_i) \) and \( \phi_2(\theta_i), i = 1, 2, 3 \), are not all in \((-\pi, \pi)\) is when one of the incoming signals is from the direction parallel to a line on which the two sensors with spacing \( \frac{1}{2} \) are located. The other two signals can be either from the opposite direction or from other directions. If one of the other two signals is from the opposite direction, it can be easily proved that the corresponding steering matrix is full rank. If the other two signals are from the two other different directions, then one of \( \phi_n(\theta_i), n = 1, 2, i = 1, 2, 3 \) is equal to \( \pi \) and the rest are real numbers from \((-\pi, \pi)\). Similarly, we can prove that the matrix \( V \) is of full rank.

**Only if part:**

If the conditions in Theorem 1 are not satisfied, rank-1 or rank-2 ambiguity occurs for some incoming signals. These situations are shown schematically in Fig.2(a)(b). In Fig.2(a), the relation between \( \theta \) and \( \alpha \) is

\[
2\pi \frac{d}{\lambda} \sin(\theta - \alpha) + k2\pi = 2\pi \frac{d}{\lambda} \sin(\theta + \alpha) \quad k \in \{1, 2, \cdots \}. \tag{50}
\]

In Fig.2(b), the relation between \( \theta \) and \( \alpha \) is

\[
2\pi \frac{d}{\lambda} \sin(\alpha) + k2\pi = 2\pi \frac{d}{\lambda} \sin\left(\frac{\pi}{2} - \theta\right), \quad k \in \{1, 2, \cdots \}. \tag{51}
\]

**Acknowledgment**

Fruitful discussions with C. C. Martin at AT&T Bell Labs are gratefully acknowledged.
References


Figure 1: Orientational invariance sensor array geometry

Figure 2: Three-sensor array structures that can cause ambiguities
Figure 3: high order array structures that can cause ambiguities
Figure 4: (a) A sixty four-sensor dense square array with four overlapping dense square subarrays of forty nine-sensors (b) A sixty four-sensor hollow square array with four overlapping hollow square subarrays of thirty two-sensors

Figure 5: A sixty four-sensor hollow square array is used in (a) and (c), A sixty four-sensor dense square array is used in (b) and (d)

Figure 6: Beamwidth comparison between a dense square array and a hollow square array (a) two DOAs are 10° apart (b) two DOAs are 5° apart
Figure 7: A nine-sensor square array with spacing $d$

Figure 8: SS and MUSIC for DOA estimation of two coherent signals at $70^\circ$ and $85^\circ$

Figure 9: Beamwidth comparison between a six-sensor linear array and a four-sensor square array
Figure 10: Standard deviation of DOA estimation using SS and FBSS

Figure 11: Multiuser Frequency Selective Channel

Figure 12: DOA estimation of four groups of coherent signals at (20°, 65°, 150°, 200°), (230°, 250°, 280°), (30°, 300°) and 320° based on a sixty four-sensor square array
Figure 13: DOA estimation of two coherent signals at an azimuth of 40° and an elevation of 30°, and at an azimuth of 50° and an elevation of 60°, respectively.

Figure 14: A twelve-sensor rectangle array with spacing $d$.

Figure 15: FBSS and ESPRIT for DOA estimation of two coherent signals at 70° and 80°.